



## 16-BIT, HIGH-SPEED, LOW-NOISE, VOLTAGE OUTPUT, DIGITAL-TO-ANALOG CONVERTER

### FEATURES

- 16-Bit Monotonic
- $\pm 5$ -V Rail-to-Rail Output
- Fast Settling: 0.65  $\mu$ s
- Fast Slew Rate: 35 V/ $\mu$ s
- Low Noise: 20 nV/ $\sqrt{\text{Hz}}$
- Low Glitch Energy: 0.5 nV-s
- Low Power-On Transient
- On-Chip Digital Low-Pass Filter
- Programmable Oversampling
- 16-MSPS Update Rate (Filter On)
- 30-MHz Serial Interface
- 1.8-V to 5.5-V Logic Compatible
- TSSOP-16 Package

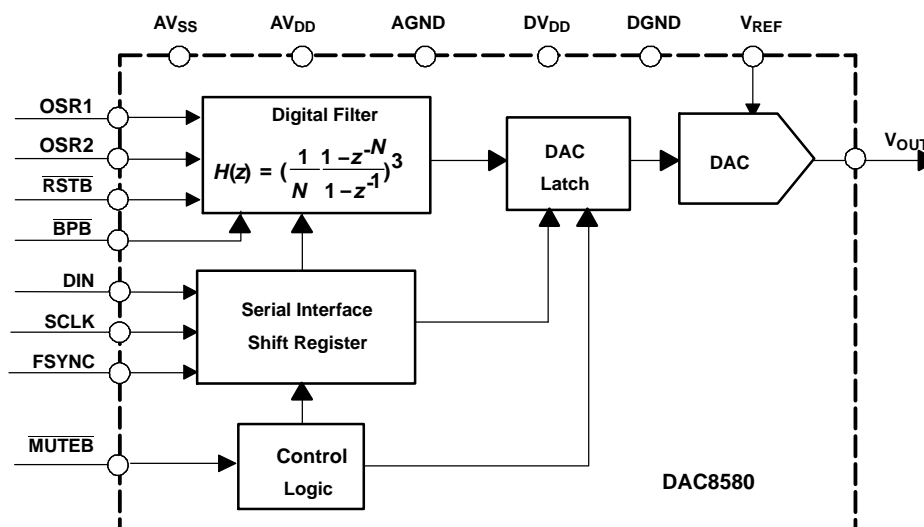
### DESCRIPTION

The DAC8580 is a 16-bit, high-speed, low-noise, voltage-output DAC designed for waveform generation applications. It operates from dual  $\pm 5$ -V power supplies and requires only a single external reference. The DAC8580 is capable of generating output signal frequencies up to 1 MHz. The DAC8580 significantly relaxes, or removes, the need for external de-glitchers, analog filters and high-swing output buffers. It incorporates a programmable digital interpolation filter capable of oversampling the input word rate by 2, 4, 8, or 16. The digital filter can be bypassed on-the-fly, or can be permanently turned off. The fast 30-MHz serial interface is compatible with right-justified digital audio format. The DAC8580 is specified from  $-40^{\circ}\text{C}$  to  $85^{\circ}\text{C}$ .

### APPLICATIONS

- Waveform Generation
- CRT Projection TV Digital Convergence
- Automated Test Equipment
- Industrial Process Control
- Music Synthesis
- Ultrasound

FUNCTIONAL BLOCK DIAGRAM OF DAC8580



Please be aware that an important notice concerning availability, standard warranty, and use in critical applications of Texas Instruments semiconductor products and disclaimers thereto appears at the end of this data sheet.

This integrated circuit can be damaged by ESD. Texas Instruments recommends that all integrated circuits be handled with appropriate precautions. Failure to observe proper handling and installation procedures can cause damage.



ESD damage can range from subtle performance degradation to complete device failure. Precision integrated circuits may be more susceptible to damage because very small parametric changes could cause the device not to meet its published specifications. This device is rated at 1500 V HBM and 1000 V CDM.

### PACKAGE/ORDERING INFORMATION<sup>(1)</sup>

PRODUCT	PACKAGE	PACKAGE DRAWING NUMBER	SPECIFICATION TEMPERATURE RANGE	PACKAGE MARKING	ORDERING NUMBER	TRANSPORT MEDIA
DAC8580	16-TSSOP	PW	–40°C TO +85°C	D8580I	DAC8580IPW	90-Piece Tube
					DAC8580IPWR	2000-Piece Tape and Reel

(1) For the most current package and ordering information, see the Package Option Addendum at the end of this document, or see the TI Web site at [www.ti.com](http://www.ti.com).

### ABSOLUTE MAXIMUM RATINGS<sup>(1)</sup>

$AV_{DD}$ or $DV_{DD}$ to $AV_{SS}$	–0.3 V to 12 V
Digital input voltage to $AV_{SS}$	–0.3 V to 12 V
$V_{OUT}$ or $V_{REF}$ to $AV_{SS}$	–0.3 V to 12 V
DGND and AGND to $AV_{SS}$	–0.3 V to 6 V
Operating temperature range	– 40°C to +85°C
Storage temperature range	– 65°C to +150°C
Junction temperature range ( $T_J$ max)	+150°C
Power dissipation: Thermal impedance ( $\theta_{JA}$ )	118°C/W
Thermal impedance ( $\theta_{JC}$ )	29°C/W
Lead temperature, soldering: Vapor phase (60 s)	215°C
Infrared (15 s)	220°C

(1) Stresses above those listed under Absolute Maximum Ratings may cause permanent damage to the device. Exposure to absolute maximum conditions for extended periods may affect device reliability.

### ELECTRICAL CHARACTERISTICS

All specifications at  $T_A = T_{MIN}$  to  $T_{MAX}$ ,  $+AV_{DD} = +5$  V,  $-AV_{DD} = -5$  V,  $DV_{DD} = +5$  V,  $V_{REF} = 4.096$  V, unless otherwise noted

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT
<b>STATIC PERFORMANCE</b>					
Resolution		16			Bits
Linearity error			±0.05		% FSR
Differential linearity error			±0.25	±1	LSB
Gain error		1	2	3	% FSR
Gain drift			±3		ppm/°C
Bipolar zero error	$V_{REF} = 4.096$ V		±5	±25	mV
Bipolar zero drift	From –40°C to +85°C		±20		µV/°C
Total drift	From –40°C to +85°C		±8		ppm/°C
<b>OUTPUT CHARACTERISTICS</b>					
Voltage output range	$AV_{DD} = 6$ V, $AV_{SS} = -6$ V, $V_{REF} = 5.5$ V	–5.5		5.5	V
Maximum current drive capability	At full speed, driving resistive load <sup>(1)</sup>		±25		mA
Output Impedance			18		Ω

(1) Sourcing and sinking dc currents larger than 25 mA is not recommended.

**ELECTRICAL CHARACTERISTICS (continued)**

All specifications at  $T_A = T_{MIN}$  to  $T_{MAX}$ ,  $+AV_{DD} = +5\text{ V}$ ,  $-AV_{DD} = -5\text{ V}$ ,  $DV_{DD} = +5\text{ V}$ ,  $V_{REF} = 4.096\text{ V}$ , unless otherwise noted

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT
Settling time (large signal)	$C_L < 200\text{ pF}$ , $R_L = 2\text{ k}\Omega$ , to 0.1% FS, 8-V step		0.35	0.65	$\mu\text{s}$
	To 0.003% FS, 8-V step		1.0		
Settling time (small signal)	To 0.003% FS, 100-mV step		0.15		$\mu\text{s}$
Slew rate	From 10% to 90% of % FSR		35		$\text{V}/\mu\text{s}$
Code-to-code glitch impulse	1 LSB change around major carry		5		mV
Code-to-code glitch energy	1 LSB change around major carry		0.5		nV-s
Overshoot	Limited by slew-boost circuit operation during large-signal swings.		100		mV
Digital feedthrough <sup>(2)</sup>	SCLK toggling		0.5		nV-s
Voltage output noise	Frequency = 100 kHz		20		$\text{nV}/\sqrt{\text{Hz}}$
	Frequency = 10 kHz		25		$\text{nV}/\sqrt{\text{Hz}}$
	F = 0.1 Hz to 10 Hz		25		$\mu\text{Vp-p}$
Power supply rejection	$V_{DD}$ varies $\pm 10\%$		0.3		$\text{mV}/\text{V}$
<b>REFERENCE INPUT CHARACTERISTICS</b>					
Reference input voltage range		3.0		$AV_{DD}$	V
Reference input impedance			5		$\text{k}\Omega$
Reference input capacitance			5		pF
Reference multiplying bandwidth	Large signal (1 V peak-to-peak)		3		MHz
Reference multiplying bandwidth	Small signal		10		MHz
<b>AC CHARACTERISTICS</b>					
2 <sup>nd</sup> Harmonic distortion	DAC output signal (sine wave) frequency = 1 kHz, DAC input update rate = 192 KSPS, Digital filter is OFF		-72		dB
	DAC output signal (sine wave) frequency = 40 kHz, DAC input update rate = 1 MSPS, Digital filter oversampling rate = 16 <sup>(3)</sup>		-72	-56	
	DAC output signal (sine wave) frequency = 1 kHz, DAC input update rate = 192 KSPS, Software calibrated, digital filter is OFF <sup>(4)</sup>		-100		
3 <sup>rd</sup> Harmonic distortion	DAC output signal (sine wave) frequency = 1 kHz, DAC input update rate = 192 KSPS, Digital filter is OFF		-72		dB
	DAC output signal (sine wave) frequency = 40 kHz, DAC input update rate = 1 MSPS, Digital filter oversampling rate = 16 <sup>(3)</sup>		-72	-56	
	DAC output signal (sine wave) frequency = 1 kHz, DAC input update rate = 192 KSPS, Software calibrated, digital filter is OFF <sup>(4)</sup>		-100		
Spurious free dynamic range (SFDR)	DAC output signal (sine wave) frequency = 1 kHz, DAC input update rate = 192 KSPS, Digital filter is OFF		72		dB
	DAC output signal (sine wave) frequency = 40 kHz, DAC input update rate = 1 MSPS, Digital filter oversampling rate = 16 <sup>(3)</sup>	56	70		dB
	DAC output signal (sine wave) frequency = 1 kHz, DAC input update rate = 192 KSPS, Software calibrated, digital filter is OFF <sup>(4)</sup>		-100		

(2) Digital feedthrough error is defined as the area of the impulse injected into the analog output from the digital input, during the toggling of the digital input.

(3) No analog filter is used. On-chip digital filter is set at oversampling ratio of 16. High-speed digitizer has 10-MHz input bandwidth. This specification is 100% tested during production.

(4) Software calibration requires the user to calibrate the linearity error using a precision digitizer and provide the DAC inputs from a lookup table.

**ELECTRICAL CHARACTERISTICS (continued)**

All specifications at  $T_A = T_{MIN}$  to  $T_{MAX}$ ,  $+AV_{DD} = +5\text{ V}$ ,  $-AV_{DD} = -5\text{ V}$ ,  $DV_{DD} = +5\text{ V}$ ,  $V_{REF} = 4.096\text{ V}$ , unless otherwise noted

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT
Total harmonic distortion (THD)	DAC output signal (sine wave) frequency = 1 kHz, DAC input update rate = 192 KSPS, Digital filter is OFF		-70		dB
	DAC output signal (sine wave) frequency = 40 kHz, DAC input update rate = 1 MSPS, Digital filter oversampling rate = 16 <sup>(3)</sup>		-68	-56	
	DAC output signal (sine wave) frequency = 1 kHz, DAC input update rate = 192 KSPS, Software calibrated, digital filter is OFF <sup>(4)</sup>		-98		
Signal to noise ratio (SNR)	DAC output signal is 1-kHz sine wave, -1 dBFS. Noise bandwidth is from 0 to 10 kHz. <sup>(5)</sup>		110		dBFS
Maximum output frequency (without external analog filter)	Serial clock = 16 MHz, Digital filter oversampling rate = 16 THD > 50 dBs, without analog filter		0.2		MHz
Maximum output frequency (with external analog filter)	Serial clock = 32 MHz, Digital filter oversampling rate = 8 <sup>(6)</sup> THD > 50 dBs, with analog filter		1		MHz
Maximum output update rate				16	MHz
<b>DIGITAL INPUT CHARACTERISTICS</b>					
$V_{IH}$		$0.7 \times DV_{DD}$		$DV_{DD}$	V
$V_{IL}$		GND		$0.3 \times DV_{DD}$	
Input leakage current			$\pm 0.05$	$\pm 1$	$\mu\text{A}$
Input capacitance				5	pF
Power-on delay	From $V_{DD}$ high to $\overline{CS}$ low		130		$\mu\text{s}$
<b>POWER SUPPLY CHARACTERISTICS</b>					
$+AV_{DD}$		4.0	5	6.0	V
$-AV_{DD}$		-6.0	-5	-4.0	V
$DV_{DD}$		1.8		$AV_{DD}$	V
$I_{DD}$	$AV_{DD} = 5.0\text{ V}$ , $AV_{SS} = -5.0\text{ V}$ , $V_{REF} = 4.096\text{ V}$ , $I_{REF}$ included		17	24	mA
$I_{SS}$			-23	-32	
<b>TEMPERATURE RANGE</b>					
Specified performance		-40		85	$^{\circ}\text{C}$

(5) A precision delta-sigma digitizer is used to make the measurement.

(6) An oversampling ratio of 16X cannot be supported at 32 MHz clock frequency. 8X oversampling can be used instead to generate a 1-MHz output. To generate output frequencies over 200 kHz, use of analog anti-imaging filters are highly recommended. The DAC8580 digital filter still relaxes the analog filter requirements. At  $F_{OUT} > 200\text{ kHz}$ , large-signal waveforms have overshoot/undershoot due to the settling characteristics of the output amplifiers. Small-signal waveforms don't show this behavior.

**TIMING CHARACTERISTICS**

At  $-40^{\circ}\text{C}$  to  $85^{\circ}\text{C}$ ,  $DV_{DD} = +5\text{ V}$ ,  $+AV_{DD} = +5\text{ V}$ ,  $-AV_{DD} = -5\text{ V}$ , unless otherwise noted<sup>(1)(2)</sup>

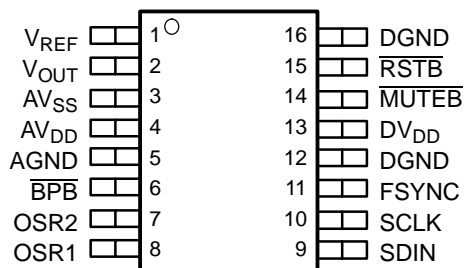
PARAMETER	MIN	MAX	UNIT
$t_{sck}$ SCLK period	33		ns
$t_{wsck}$ SCLK high or low time	16		
$t_{su}$ Data setup time (input)	5		
$t_{hi}$ Data hold time (input)	5		
$t_{SWF}$ FSYNC setup time	5		
$t_{HWF}$ FSYNC hold time	5		
$t_r$ Rise time	20	1	
$t_f$ Fall time	20	1	
$t_{WFUPDAC}$ Delay from falling edge of $\overline{FSYNC}$ to loading DAC latch <sup>(3)</sup>	1.5		$t_{sck}$

(1) Specified by design. Not production tested.

(2) Sample tested during the initial release and after any redesign or process changes that may affect this parameter.

(3) OUTPUT of pin  $V_{OUT}$  changes to new level immediately (within settling time) after DAC register is loaded.

**TSSOP PACKAGE  
(TOP VIEW)**



**TERMINAL FUNCTIONS**

NO.	NAME	DESCRIPTION
1	V <sub>REF</sub>	Reference input voltage; 3 V to AV <sub>DD</sub> .
2	V <sub>OUT</sub>	DAC output voltage; output swing is ±V <sub>REF</sub>
3	AV <sub>SS</sub>	Negative analog supply voltage; tie to –5 V
4	AV <sub>DD</sub>	Positive analog supply voltage; tie to +5 V
5	AGND	Ground reference for analog circuitry of the device
6	BPB	Active-low, asynchronous digital input for filter bypass
7	OSR2	Digital input for selecting the oversampling ratio
8	OSR1	Digital input for selecting the oversampling ratio
9	DIN	Digital input, serial data
10	SCLK	Digital input, serial bit clock
11	FSYNC	Digital input. FSYNC is word clock.
12	DGND	Ground reference for digital circuitry
13	DV <sub>DD</sub>	Positive digital supply, 1.8-V to 5.5-V compatible
14	MUTE <sub>B</sub>	Digital input, active low, for forcing the output to mid-scale.
15	RST <sub>B</sub>	Filter reset. Active-low, asynchronous digital input for disabling all digital filter activity.
16	DGND	Must connect to digital ground reference to ensure correct operation.

### RIGHT-JUSTIFIED AUDIO TIMING DIAGRAM

The DAC8580 serial interface timing uses a single channel (mono) version of right-justified audio format. The input data is latched into the device input shift register on the rising edge of SCLK, MSB first. The falling edge of FSYNC latches the last 16 bits of received data (right-justified) from the shift register into a temporary register, which connects to either the digital filter or the DAC latch. Data in the temporary register is transferred to the DAC latch (when digital filter is off), or to the digital filter (when the filter is on) on the second rising SCLK edge after the falling edge of FSYNC. For operating the digital filter, a continuous SCLK is required.

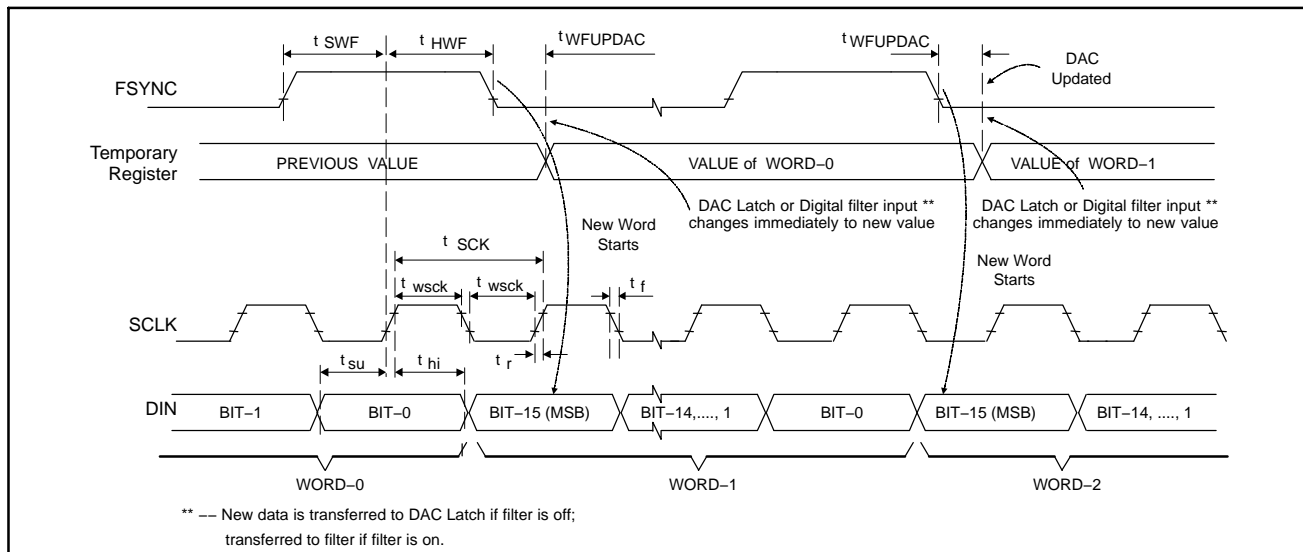


Figure 1. Timing Diagram

### TYPICAL CHARACTERISTICS (AVDD = 5 V, AVSS = -5 V, VREF = 4.096 V, unless otherwise noted)

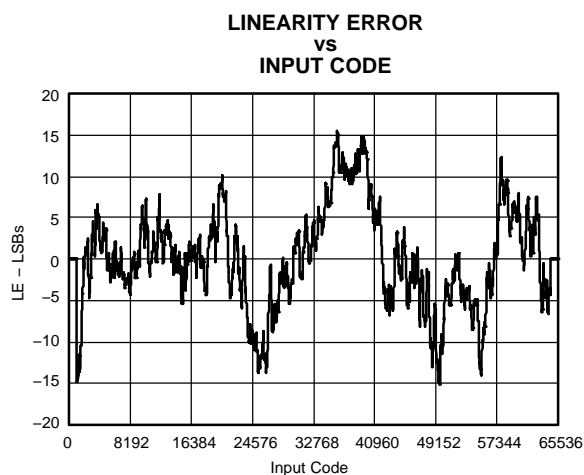


Figure 2.

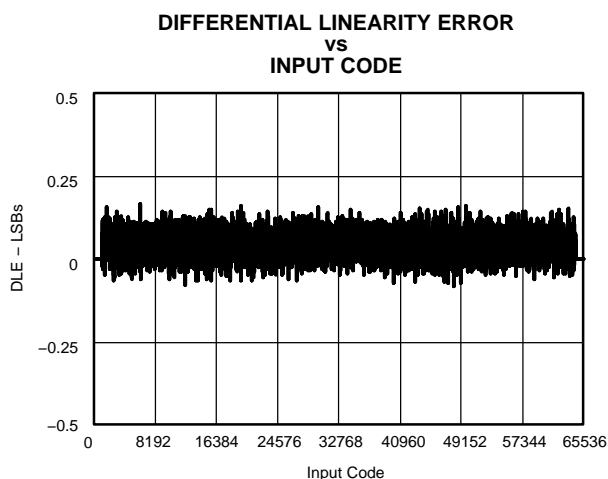


Figure 3.

**TYPICAL CHARACTERISTICS (AVDD = 5 V, AVSS = -5 V, VREF = 4.096 V, unless otherwise noted) (continued)**

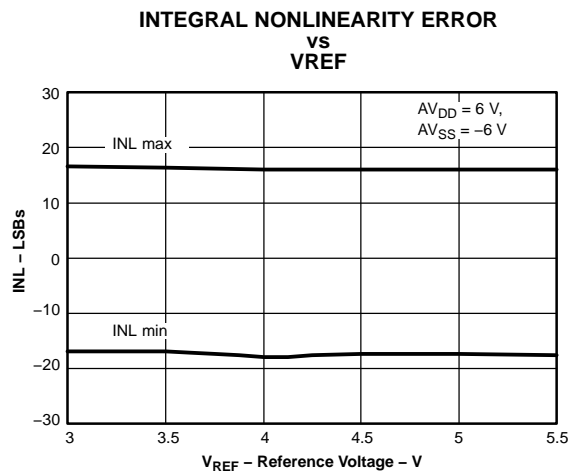


Figure 4.

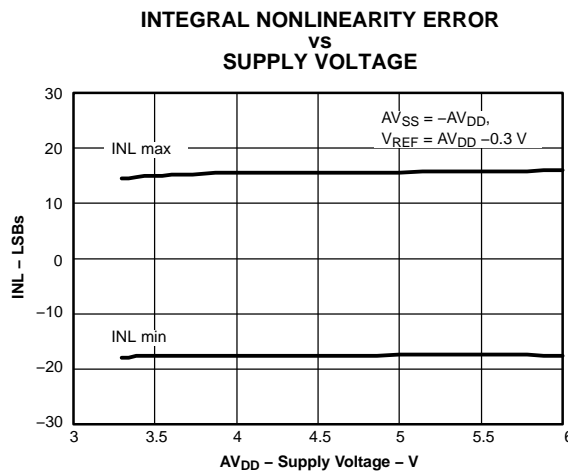


Figure 5.

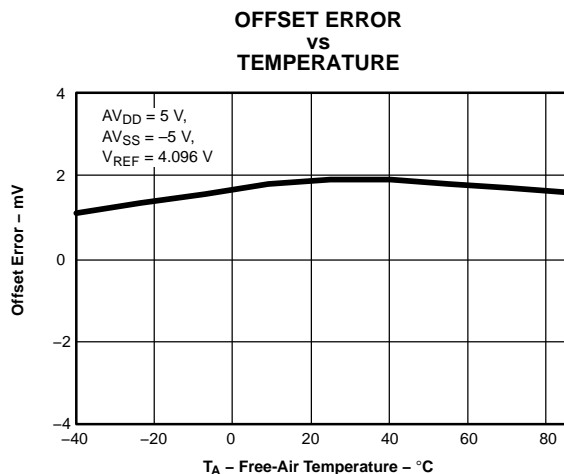


Figure 6.

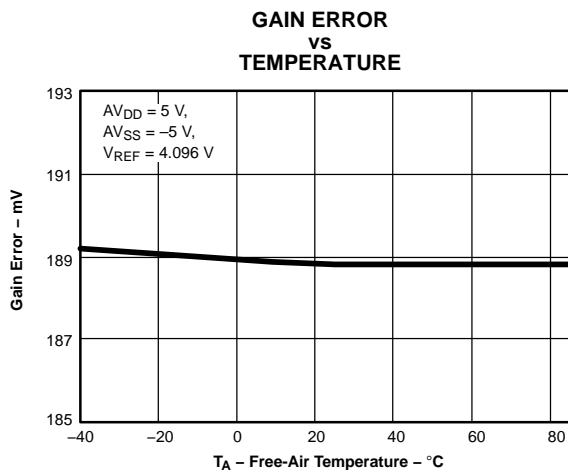


Figure 7.

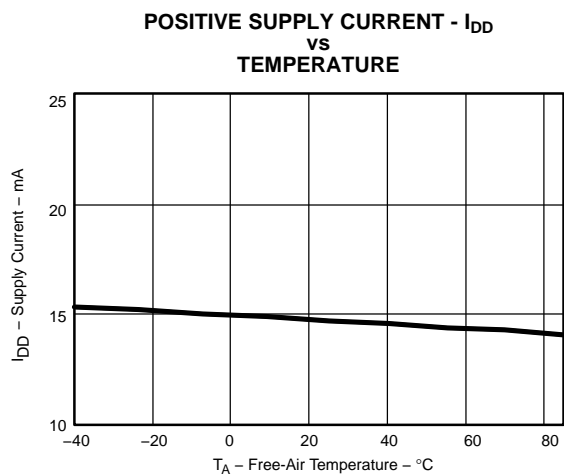


Figure 8.

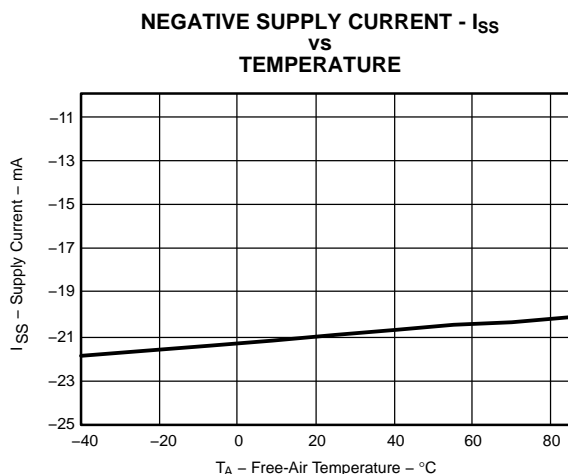


Figure 9.

**TYPICAL CHARACTERISTICS (AVDD = 5 V, AVSS = -5 V, VREF = 4.096 V, unless otherwise noted) (continued)**

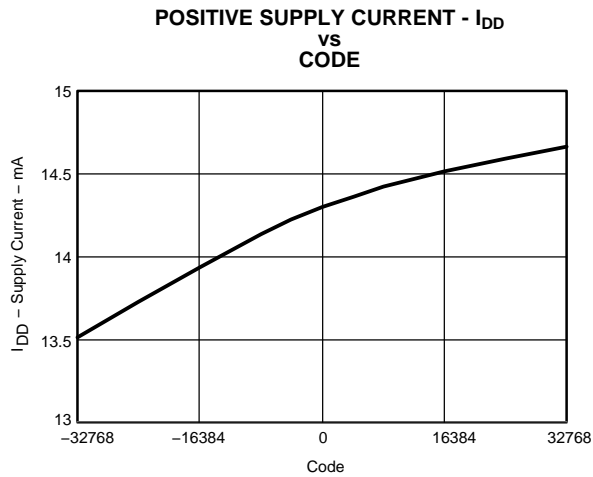


Figure 10.

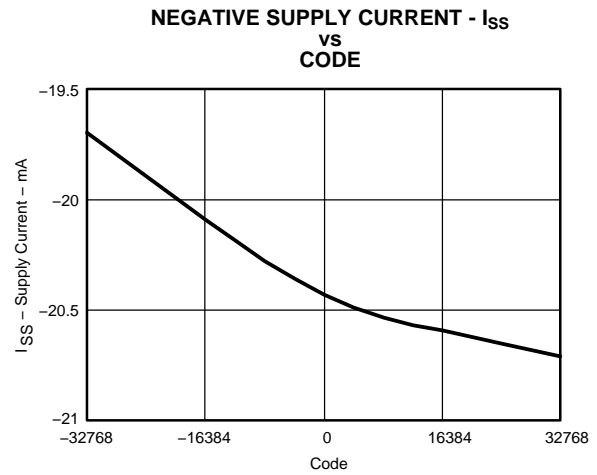


Figure 11.

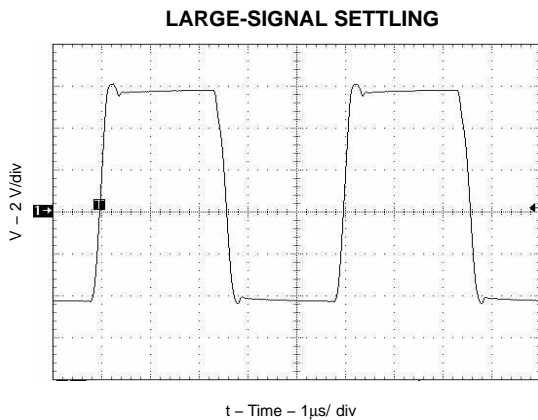


Figure 12.

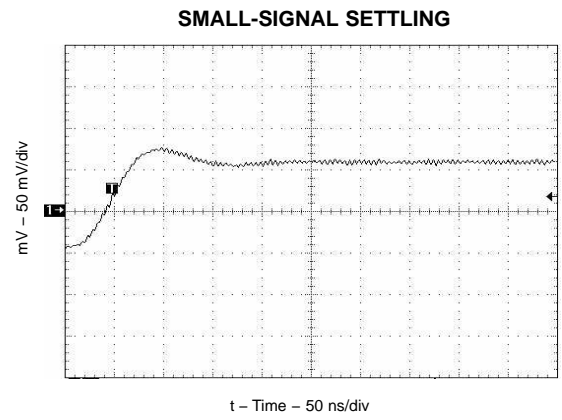


Figure 13.

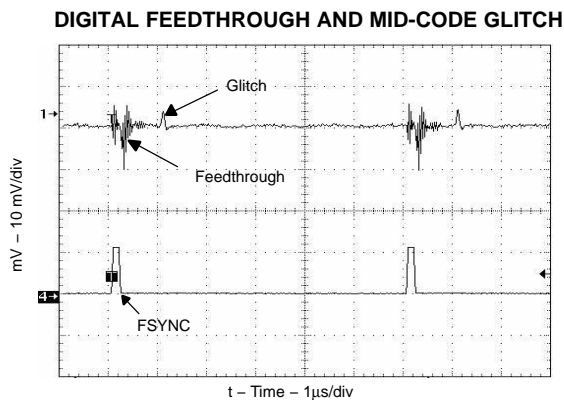


Figure 14.

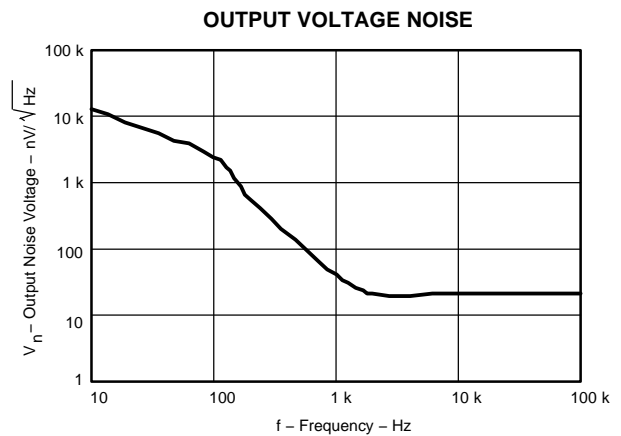


Figure 15.



**TYPICAL CHARACTERISTICS (AVDD = 5 V, AVSS = -5 V, VREF = 4.096 V, unless otherwise noted) (continued)**

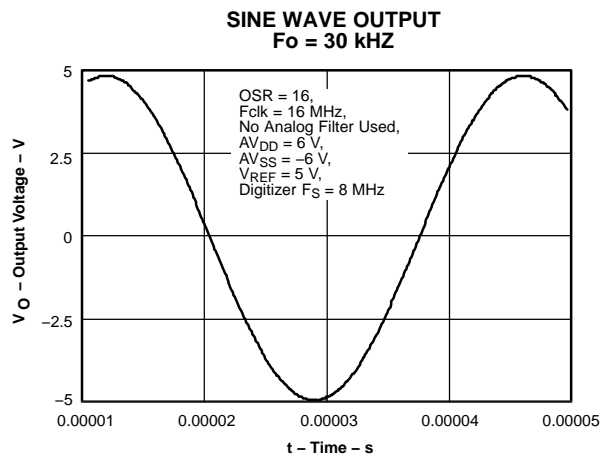


Figure 16.

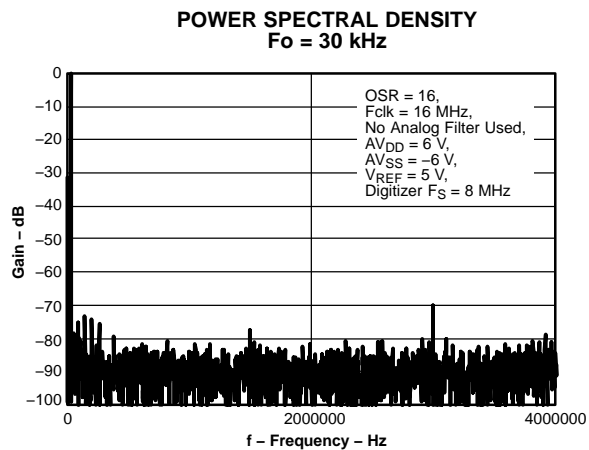


Figure 17.

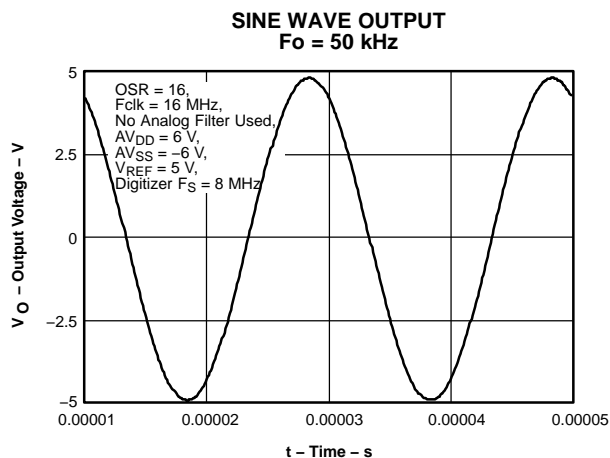


Figure 18.

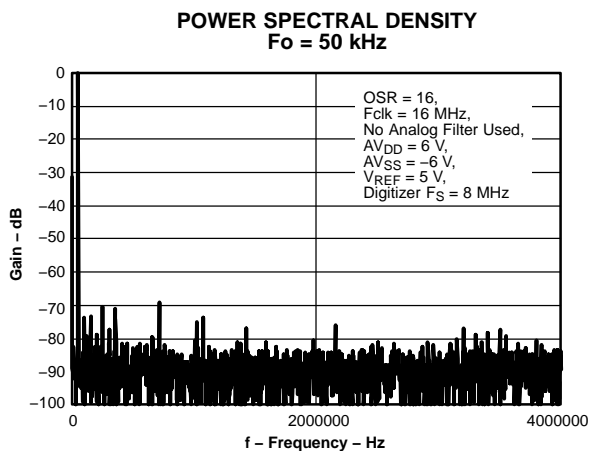


Figure 19.

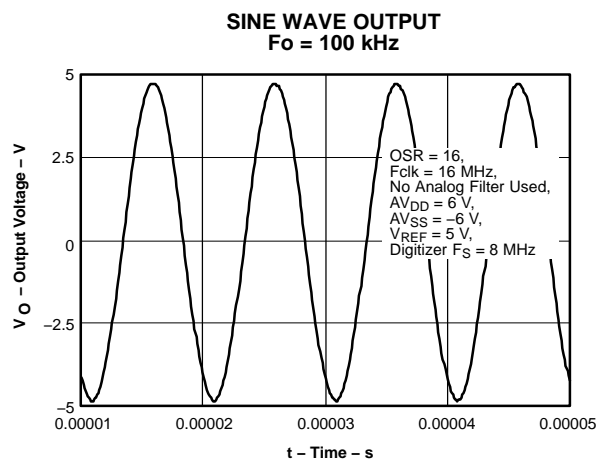


Figure 20.

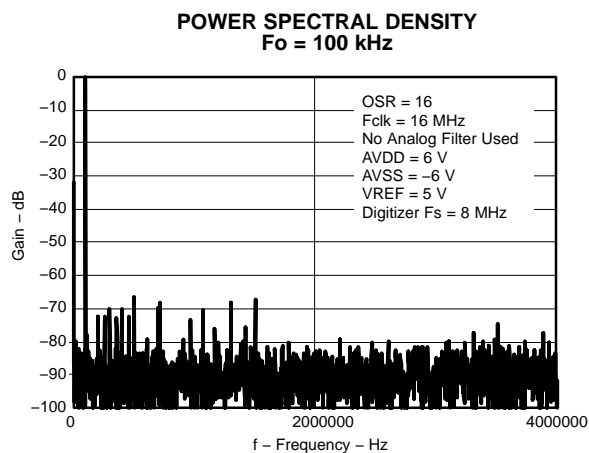


Figure 21.

**TYPICAL CHARACTERISTICS (AVDD = 5 V, AVSS = -5 V, VREF = 4.096 V, unless otherwise noted) (continued)**

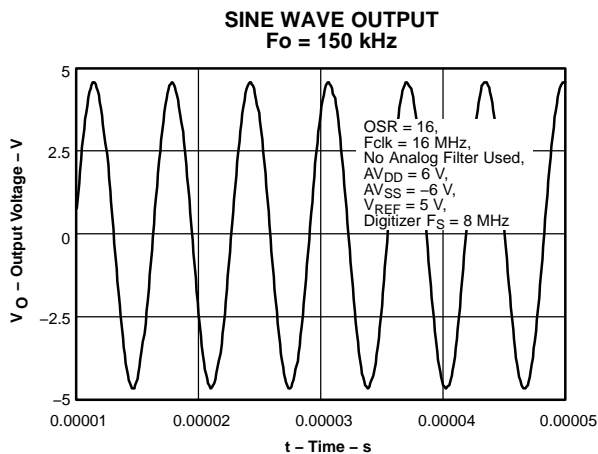


Figure 22.

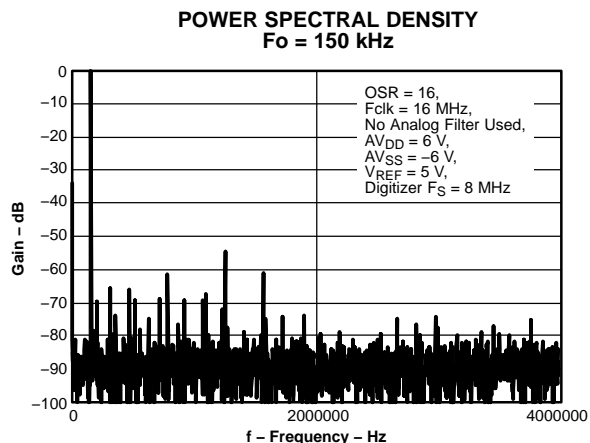


Figure 23.

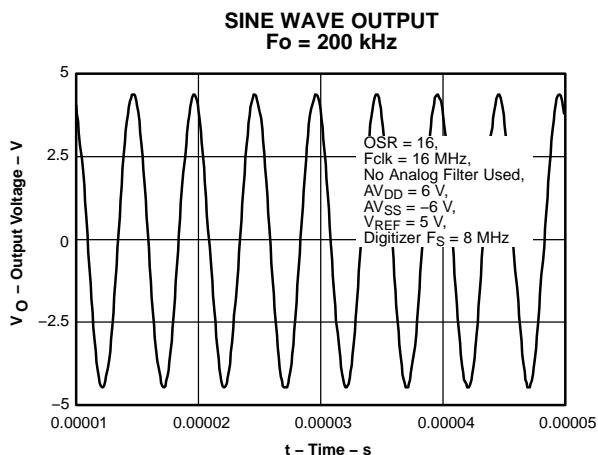


Figure 24.

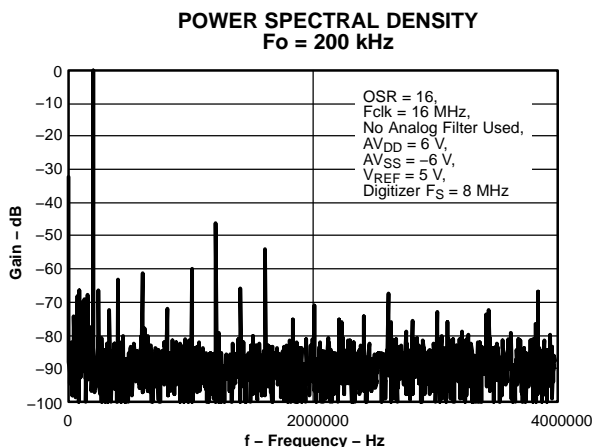


Figure 25.

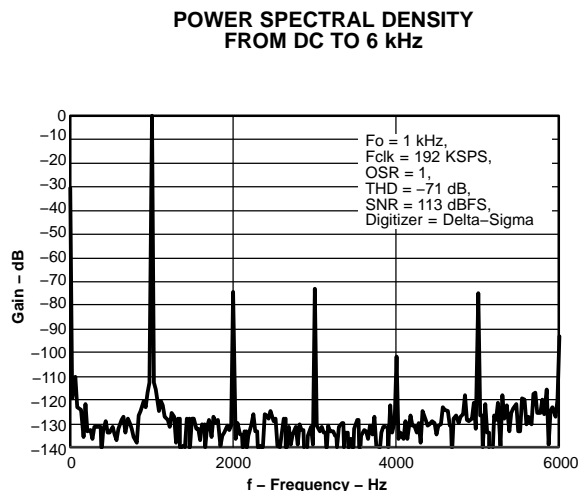


Figure 26.

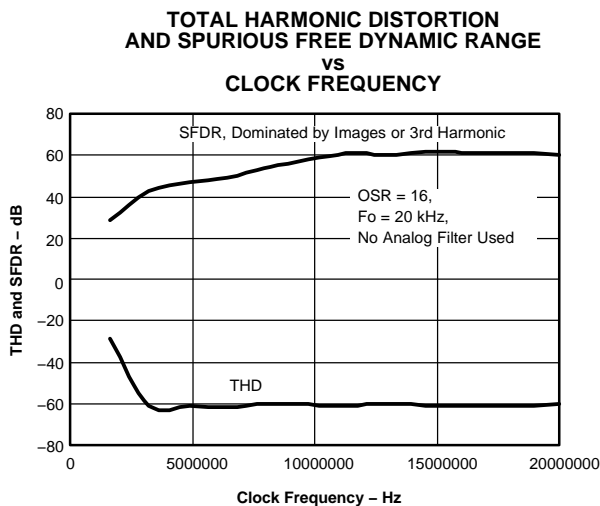


Figure 27.

**TYPICAL CHARACTERISTICS (AVDD = 5 V, AVSS = -5 V, VREF = 4.096 V, unless otherwise noted) (continued)**

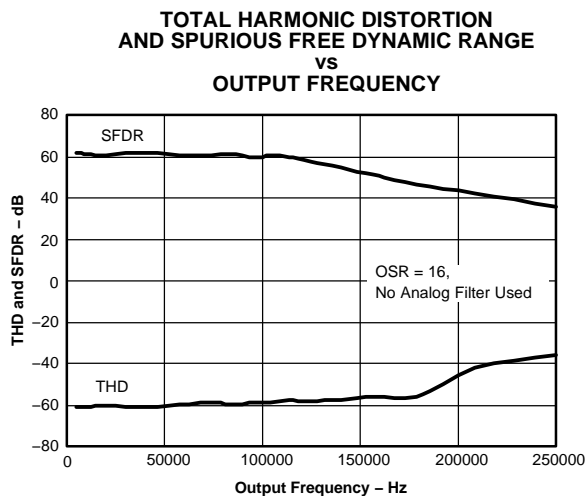


Figure 28.

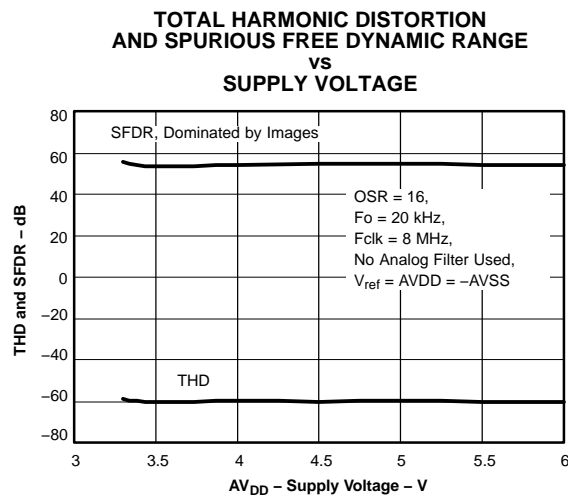


Figure 29.

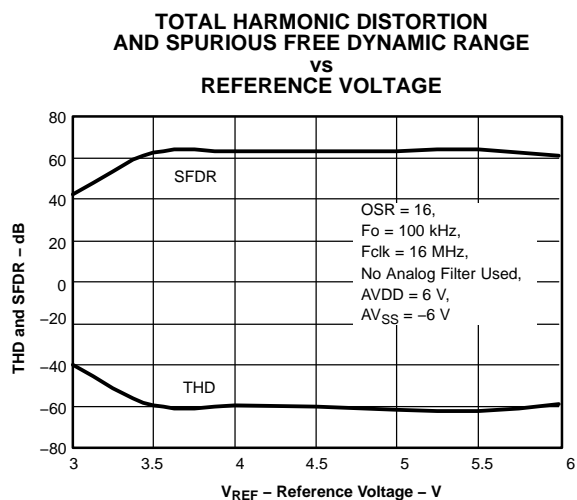


Figure 30.

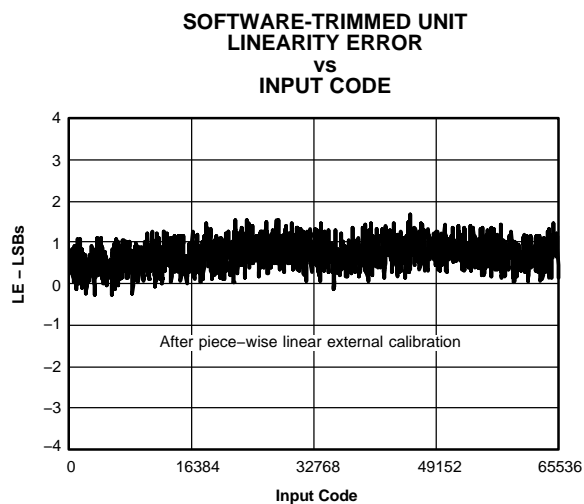


Figure 31.

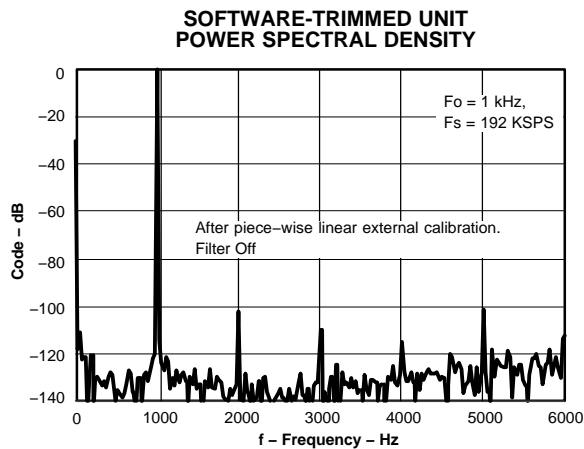
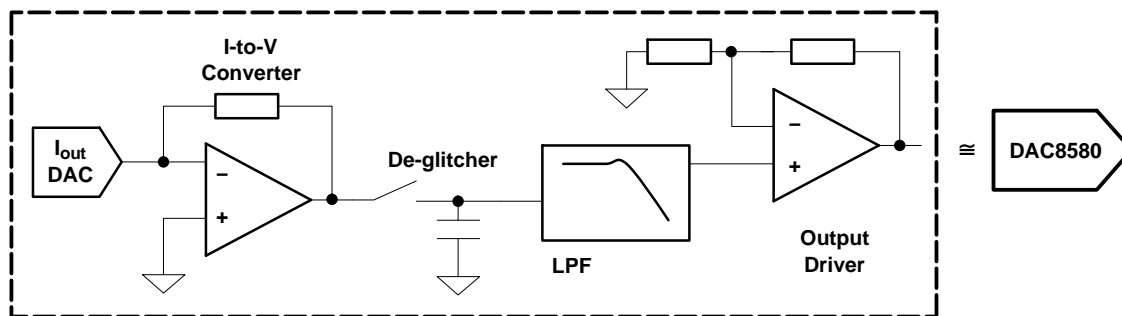


Figure 32.

## THEORY OF OPERATION

The traditional high-speed, voltage-output D/A conversion employs a current-output DAC followed by an I-to-V conversion amplifier. For voltage waveform generation applications, these components are typically followed by a sample-and-hold de-glitcher circuit, an analog low-pass filter, and an external buffer to drive low-impedance loads (see Figure 33). Monolithic applications of such traditional architectures suffer from the imperfections of on-chip sample-and-hold circuits, and the analog filters. Multi-chip applications of this traditional architecture suffer from voltage drift problems due to the temperature coefficient mismatches between external passive components and the D/A converter, as well as large circuit size and high cost. DAC8580 is designed to address the problems of traditional high-speed, high-resolution, voltage-output D/A converters.



**Figure 33. Traditional Voltage Output Waveform Generation Circuitry Replaced by a Single DAC8580**

The DAC8580 uses a proprietary, inherently monotonic, high-speed, low-glitch, resistor-string architecture, followed by an on-chip low-noise output amplifier. 16-bit input data is coded in twos-complement format and transmitted using a 3-wire serial interface (MSB first). The input data is sent to an on-chip digital interpolation filter. The filter can be programmed to different oversampling rates, it can be bypassed, or it can be totally disabled. The digital data is then decoded to select a tap voltage of the resistor string. The resistor-string output is sent to a high-speed, low-noise output amplifier. The output buffer has quasi-rail-to-rail swing capability (within 250-mV range of each rail) on a 600- $\Omega$ , 200-pF load. Loads of 50  $\Omega$  or 75  $\Omega$  can also be continuously driven as long as the output current remains within  $\pm 25$  mA. The DAC8580 reduces the components that are used for implementing sample-and-hold circuits, analog filters, and output driver amplifiers.

The resistor-string DAC architecture provides low glitch, exceptional differential linearity, and temperature stability while the output buffer provides fast settling and exceptionally low noise (20 nV/ $\sqrt{\text{Hz}}$ ). The DAC8580 settles well under 1  $\mu\text{s}$  for large signals. The small-signal settling time is less than 150 ns, which enables (oversampled) update rates exceeding 6.7 MSPS. If some small-signal settling error can be tolerated, the DAC8580 can update as fast as 16 MSPS.

Due to the remarkably low glitch energy, the DAC8580 has low harmonic distortion (–70 dB THD for 1-kHz sine wave output). When the linearity error of the DAC8580 is calibrated using a lookup table, the THD performance typically exceeds 98 dBs, without an external S/H circuit.

The DAC8580 needs a low-noise external reference voltage to set its output voltage range. The DAC8580 does not introduce glitches to the external voltage source. This significantly reduces the crosstalk when a single external reference is used to supply the reference voltage for multiple devices.

The DAC8580 has a 3-wire serial interface to communicate with a microprocessor or a DSP. The host is not overloaded by the DAC8580: When the digital filter is on, the host needs only to send 1-out-of-16 data points (for oversampling rate 16). The digital filter of the DAC8580 can generate the remaining data points digitally, on-chip. When the digital filter is disabled (bypassed), the DAC8580 operates as a standard, 16-bit, 2-MSPS, voltage-output DAC. The 1.8-V to 5.5-V digital interface of the DAC8580 enables compatibility with various logic families.

### Output Voltage ( $V_{\text{OUT}}$ )

The DAC8580 uses a high-performance rail-to-rail output buffer capable of driving a 600- $\Omega$ , 200-pF load with fast 1- $\mu\text{s}$  large-signal settling. The buffer has exceptional noise performance (20 nV/ $\sqrt{\text{Hz}}$ ) and fast slew-rate (35 V/ $\mu\text{s}$ ). The small-signal settling time is under 150 ns, supporting DAC update rates exceeding 6.7 MSPS.

## THEORY OF OPERATION (continued)

On power up, a switching circuitry is used to lower power-on transients. Before power up, the DAC output is connected to AGND voltage using a 100-k $\Omega$  resistor. During power up, transient output voltages are typically less than 200 mV. Approximately 30  $\mu$ s after power up, the output gets set to mid-scale value (power-on reset). This mid-scale value is around AGND potential within offset error limits.

**Table 1. Two's-Complement Data Format**

DAC OUTPUT	DIGITAL CODE	
	BINARY	HEX
+Vref	0111111111111111	7FFF
+Vref/2	0100000000000000	4FFF
0	0000000000000000	0000
-Vref/2	1011111111111111	BFFF
-Vref	1000000000000000	8000

### Reference Input Voltage ( $V_{REF}$ )

The reference input pin VREF is typically tied to a standard 3-V, 4.096-V, or 5-V external reference. Minimum external reference voltage that can be used is 3 V. A 0.1- $\mu$ F (or less) bypass capacitor is recommended, depending on the load-driving capability of the external voltage reference. To reduce crosstalk and improve settling time, VREF pin is internally buffered by a high-performance amplifier. Pin VREF has a constant 5-k $\Omega$  impedance to AGND; therefore, a reference driver should be chosen with care. Because the VREF pin does not induce glitches, multiple DAC8580 devices can share a single external reference without crosstalk concerns. In addition, because the reference pin does not require fast current spikes, the reference voltage generator can be heavily filtered to improve noise performance without hurting settling or distortion. The output range of the DAC8580 is equal to  $\pm V_{REF}$ . Pin VREF should not be powered before the supply pins. REF3133 and REF3140 are recommended to set the DAC8580 output range to  $\pm 3.3$  V and  $\pm 4.096$  V, respectively. The reference bandwidth is 10 MHz (small signal) and 3 MHz (large signal).

### Power Supply ( $AV_{DD}$ , $AV_{SS}$ , $DV_{DD}$ )

The DAC8580 uses  $\pm 5$ -V analog power supplies ( $AV_{DD}$ ,  $AV_{SS}$ ) and a 1.8-V to 5.5-V digital supply ( $DV_{DD}$ ). Analog and digital ground pins (AGND and DGND) are also provided. For low-noise operation, analog and digital power, and ground pins should be separated. Sufficient bypass capacitors, at least 1  $\mu$ F, should be placed between  $AV_{DD}$  and  $AV_{SS}$ ,  $AV_{SS}$  and DGND, and  $DV_{DD}$  and DGND pins. Series inductors are not recommended on the supply paths.  $AV_{DD}$ ,  $DV_{DD}$ ,  $AV_{SS}$ , and VREF should be applied together. VREF must not be applied before  $AV_{DD}$  and  $AV_{SS}$ . During power up, all digital inputs and the reference input should be kept at zero volts. If any pin is brought high before the power supplies, overvoltage protection circuitry turns on.

### SERIAL INTERFACE

The DAC8580 serial interface consists of serial data input pin SDIN, bit clock pin SCLK, and word clock pin FSYNC. The serial interface is designed to support the right-justified (mono) audio format. The serial inputs are 1.8-V to 5.5-V logic compatible.

Data from SDIN pin is continuously clocked into a 16-bit shift register, at each rising edge of SCLK. Falling edge of the FSYNC latches the shift register data into a 16-bit temporary register. The second rising edge of SCLK following the falling edge of FSYNC transfers the data stored in the temporary register to the DAC latch when the digital filter is turned off; when the digital filter is on, data is transferred to the digital filter. That is, DAC data is updated 1.5 clock cycles after the falling edge of FSYNC when the digital filter is off. The shift register continuously performs a shift operation; therefore, on the falling edge of the word clock FSYNC, the last 16 bits received determines the data update (right-justified). Data is received MSB-first. This operation provides a simplified timing for the digital filter, and enables clock rates exceeding 30 MHz. See the timing diagram for details.

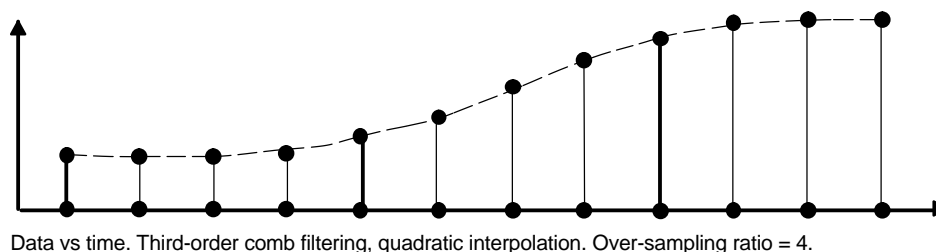
## DIGITAL FILTER

The digital filter removes, or simplifies, the component tolerance and temperature drift requirements of the analog filter that follows the DAC8580. Thus, the digital filter reduces the system cost, and improves system reliability. The filter does so at the expense of a 2-input-word delay and some rolloff of the input spectrum, which also is present for the case of an analog filter. The DAC8580 is not a delta-sigma DAC. No noise shaping is performed, and there is no out-of-band noise other than the significantly reduced image frequencies. Driving a 600- $\Omega$  load, the DAC8580 idle channel noise typically exceeds 115 dBs over the audio bandwidth.

For output signals exceeding 200 kHz, an analog anti-imaging filter is recommended.

The digital filter is a third-order comb filter with programmable oversampling ratio, which performs a second-order interpolation on the input data.

Figure 34 shows the third-order comb filter effect, which is quadratic interpolation (two-frame delay is not shown).



**Figure 34. Data vs Time – Third-Order Comb Filtering**

The digital filter has a two-frame delay, independent of the oversampling rate. It does not exactly preserve the input samples. However, it has the nice property of outputting the input sample, if two repetitive input frames are used in a row. It is a finite impulse response (FIR) filter with linear phase, and it does not distort audio phase relationships. The hardware implementation uses feedback; therefore, it is implemented similar to an infinite impulse response (IIR) filter. The number of equivalent FIR coefficients depends on the oversampling rate and is not described in detail. The filter has the following Z-transform and its low-pass frequency response has  $\sin x/x$  envelope to the third power.

$$H(z) = \left( \frac{1}{N} \frac{1 - z^{-N}}{1 - z^{-1}} \right)^3 \quad (1)$$

The filter serves three major purposes:

The first purpose of the filter is to relax the analog filtering requirement by pushing the image frequencies higher in the spectrum. A single analog RC filter, or no analog filter at all, could work fine. Image frequencies are a fundamental property of an ideal D/A converter, and they can easily dominate the spurious free dynamic range (SFDR) for high-frequency output signals. The digital filter helps remove these image frequencies. Image frequencies appear at the integer multiples of the output data update rate ( $\pm$ ) input signal rate. For example, a 1-MSPS DAC generating a 225-kHz sine wave has image frequencies pop up at 775 kHz, 1.225 MHz, 1.775 MHz, 2.25 MHz, etc. The images for the fifth-harmonic are at 112.5 kHz, 887.5 kHz, 1.125 MHz, 1.887 MHz, etc. This 112.5-kHz image for the fifth harmonic pops up even below the 225 kHz fundamental. With an oversampling rate of 16, at 16 MSPS, the image frequency for that same fifth harmonic is pushed back to  $16 \text{ MHz} - 5 \times 225 \text{ kHz} = 14.875 \text{ MHz}$ , which can be filtered easily with an RC circuit.

The second purpose of the digital filter is to relax the computational burden on the microcontroller unit driving the DAC8580. At an oversampling rate of 16, the MCU needs to generate only 1-out-of-16 samples; 15 samples out of 16 are computed and generated by the DAC8580 digital filter. Even the input sample itself gets recomputed into a slightly different value by the filter. This way a high-MIPS (million instructions per second) MCU or DSP is not required to drive the DAC8580 for continuous waveform generation applications. A simple microcontroller is sufficient.

The third purpose of the filter is to relax the burden on the DAC8580 output buffer by band limiting the digital input signal. Analog overshoot is not generated during smooth digital signals (filter on). Moreover, when the filter is on, the 150-ns small-signal settling time becomes a dominant factor, as opposed to the 1- $\mu$ s large-signal settling time. This enables 6.7-MSPS operation with full settling; 16 MSPS is possible if full settling is not necessary. At output update rates above 6.7 MSPS, the user can trade off image frequencies with distortion caused by insufficient settling.

When the filter is bypassed (pin  $\overline{\text{BPB}}$  connects to DGND), the DAC latch is loaded directly with the value from the input temporary register. The DAC output changes immediately when the input temporary register is loaded with the new value. If high-speed signals are needed within smooth signals, the filter bypass feature is useful to temporarily switch back to 35 V/ $\mu$ s fast slew rate, while the filter is still in operation.

The DAC8580 uses an infinite impulse response (IIR) implementation of the third-order comb filter. This implementation is stable when there is exactly 16 SCLK rising edges per frame. SCLK should be equally spaced, continuous, and uninterrupted for proper filtered operation. The particular frame during which the  $\overline{\text{RSTB}}$  pulse makes a low-to-high transition can contain any number of clock cycles, but after that frame, there must be 16 clocks per frame.

For oversampling ratios of 1, 2, 4, 8, and 16, the DAC8580 analog outputs change every 16, 8, 4, 2, and 1 SCLK rising edges, respectively. For all oversampling ratios, DAC8580 always receives one input data every 16 SCLK cycles. To perform the low-pass function, the digital filter uses the current input, as well as two previous inputs. During power up, when three consecutive inputs are not yet available, the current input and two previous inputs are taken at mid-scale code. The intermediate points between consecutive digital input samples are computed (interpolated) by the digital filter and sent to the output at a higher update rate determined by the oversampling ratio.

The digital filter itself can support update rates up to 16 MSPS due to inherent logic delay limitations. Therefore, the oversampled output update rate of the DAC8580 should not exceed 16 MSPS. For example:

**Case 1:** F<sub>sclk</sub> = 32 MHz

$$D_{in} = 32 \text{ MHz}/16 = 2 \text{ MSPS}$$

$$V_{out} (\text{OSR} = 2) = 4 \text{ MSPS}$$

$$V_{out} (\text{OSR} = 4) = 8 \text{ MSPS}$$

$$V_{out} (\text{OSR} = 8) = 16 \text{ MSPS}$$

$$V_{out} (\text{OSR} = 16) = \text{Not allowed, limited by the filter update-rate.}$$

**Case 2:** F<sub>sclk</sub> = 16 MHz

$$D_{in} = 16 \text{ MHz}/16 = 1 \text{ MSPS.}$$

$$V_{out} (\text{OSR} = 2) = 2 \text{ MSPS}$$

$$V_{out} (\text{OSR} = 4) = 4 \text{ MSPS}$$

$$V_{out} (\text{OSR} = 8) = 8 \text{ MSPS}$$

$$V_{out} (\text{OSR} = 16) = 16 \text{ MSPS}$$

## CONFIGURATION of DIGITAL FILTER

The digital filter is configured through hardware as shown in [Table 2](#).

**Table 2. Configuration of Digital Filter**

<b>BPB</b>	<b>RSTB</b>	<b>OSR2</b>	<b>OSR1</b>	<b>MUTE<math>\overline{B}</math></b>	<b>DESCRIPTION</b>
Don't care	Don't care	Don't care	Don't care	0	OUTPUT CLEAR. The output goes to mid-scale, 1.5 SCLK cycles after falling FSYNC
0	0	Don't care	Don't care	1	STANDARD DAC OPERATION (FILTER OFF) DAC output updates with serial data, 1.5 SCLK after falling FSYNC
1	0	Don't care	Don't care	1	FILTER INITIALIZATION Digital filter gets reset. DAC output goes to mid-scale after receiving SCLK rising edge.
0	1	Don't care	Don't care	1	STANDARD DAC OPERATION (FILTER COMPUTES IN THE BACKGROUND) DAC output updates with serial data, 1.5 SCLK after falling FSYNC
1	1	0	0	1	2X oversampled OPERATION WITH FILTER ON DAC output updates with filtered data, 1.5 SCLK after falling FSYNC and every 8 <sup>th</sup> SCLK thereafter.
1	1	0	1	1	4X oversampled OPERATION WITH FILTER ON DAC output updates with filtered data, 1.5 SCLK after falling FSYNC and every 4 <sup>th</sup> SCLK thereafter.
1	1	1	0	1	8X oversampled OPERATION WITH FILTER ON DAC output updates with filter data, 1.5 SCLK after falling FSYNC and every 2 <sup>nd</sup> SCLK thereafter.
1	1	1	1	1	16X oversampled OPERATION WITH FILTER ON DAC output updates with filter data, 1.5 SCLK after falling FSYNC and every SCLK thereafter.

### Mute Function (Pin MUTE $\overline{B}$ )

Mute function is implemented by setting the DAC output voltage to mid-scale ( $\sim 0$  V). The MUTE $\overline{B}$  pin is active low, and is synchronized with the frame. That is, the DAC latch and DAC output are immediately set to mid-scale during the first update while the MUTE $\overline{B}$  pin is low. The MUTE $\overline{B}$  pin works independent of the serial data transfer, or the digital filter. Neither the serial input, nor the digital filter data get interrupted or get lost while the output is set at mid-scale with MUTE $\overline{B}$ . The first DAC update occurring after the MUTE $\overline{B}$  pin goes high sets the DAC latch and DAC output to the next desired value. MUTE $\overline{B}$  pin must be kept at logic low level before power up.

### Oversampling Rate (Pin OSR2, OSR1)

oversampling rate of the digital filter is set via pins OSR2 and OSR1.

<b>OSR2</b>	<b>OSR1</b>	<b>OVERSAMPLING RATE</b>
0	0	2
0	1	4
1	0	8
1	1	16

The DAC8580 can support these oversampling ratios as long as the oversampled update rate does not exceed 16 MSPS. The oversampling ratio should be set at power up. OSR1 and OSR2 pins must be kept at logic-low level before power up.

### Digital Filter Bypass (Pin BPB)

The digital filter can be asynchronously bypassed via pin BPB. When pin BPB is active low, the digital filter is bypassed. In this case, the DAC latch receives the data from the temporary register, not from the digital filter. When the series input data is latched into the temporary register from the input shift register, the DAC latch and DAC output are updated immediately with the new value of the temporary register. When pin BPB is high, digital filter is not bypassed. The DAC latch is loaded with the output of the digital filter, not with the content of the temporary register. The digital filter generates the data and transfers it to the DAC latch.

When the digital filter is bypassed, the filter keeps running. A bypass does not disrupt the internal computations of the digital filter. When the BPB pin goes high, the oversampled operation resumes without any discontinuity of



the filtered output. The  $\overline{\text{BPB}}$  pin multiplexes the DAC input between the filter output and the output of the temporary register. Certain applications require generation of smooth waveforms, combined with fast edges. A good example is the CRT positioning signal, where a smooth ramp is followed by a fast blanking pulse. The digital low-pass filter offers the capability to generate smooth ramp waveforms (with filter on) and fast blanking pulse (with filter bypassed). The bypass feature offers on-the-fly capability to switch between smooth filtered operation and high-speed unfiltered operation. The  $\overline{\text{BPB}}$  pin must be kept at logic low before power up.

### Digital Filter Asynchronous Reset (Pin $\overline{\text{RSTB}}$ )

The digital filter equation is invalidated if other than 16 clocks per frame are received. This condition causes numerical instability; the  $\overline{\text{RSTB}}$  pin is used for recovering from such errors without forcing the user to issue a power-on reset. The  $\overline{\text{RSTB}}$  digital input is an active-low, asynchronous filter reset. The  $\overline{\text{RSTB}}$  does not reset the serial interface. Immediately after  $\overline{\text{RSTB}}$  becomes low, all filter registers were cleared, all filter clocks are stopped, all digital filter switching activities are stopped in order to lower switching noise and digital power consumption. If the digital filter is not needed, the  $\overline{\text{RSTB}}$  and  $\overline{\text{BPB}}$  pins should both be tied to a logic zero. The filter reset operation always occurs asynchronously when  $\overline{\text{RSTB}} = 0$ . However, the effect of  $\overline{\text{RSTB}} = 0$  at the DAC output ( $V_{\text{out}} \sim 0 \text{ V}$ ) cannot be observed if the SCLK is stopped, or if  $\overline{\text{BPB}} = 0$ . Pin  $\overline{\text{RSTB}}$  must be kept at logic low before power up.

The DAC8580 monitors for receipt of 16 clocks per frame and issues an automatic filter reset if other than 16 clocks per frame is received. This auto-reset is synchronized with the FSYNC line.

$\overline{\text{RSTB}}$	$\overline{\text{BPB}}$	OPERATION
0	0	Conventional DAC operation: Shutdown and disconnect the digital filter
0	1	Filter reset. DAC output becomes $\sim 0 \text{ V}$ only if SCLK is continuously running.
1	0	Filter bypass. Conventional DAC operation resumes, while filter is on.
1	1	Filtered operation. DAC outputs filtered data at the oversampling rate.

APPLICATION INFORMATION

CRT Projection TV Digital Convergence

The DAC8580 is an ideal component for the digital convergence units of the three-tube projection TV sets. Digital convergence applications require the generation of precision voltage waveforms with approximately 150-kHz bandwidth. Six DAC8580s are needed for one TV set to generate convergence waveforms for horizontal and vertical red, green, and blue, as seen in Figure 35. A single external reference, REF3025, can support all six DACs. The low temperature drift, low glitch, and low noise of the DAC8580 improve the picture quality and color drift.

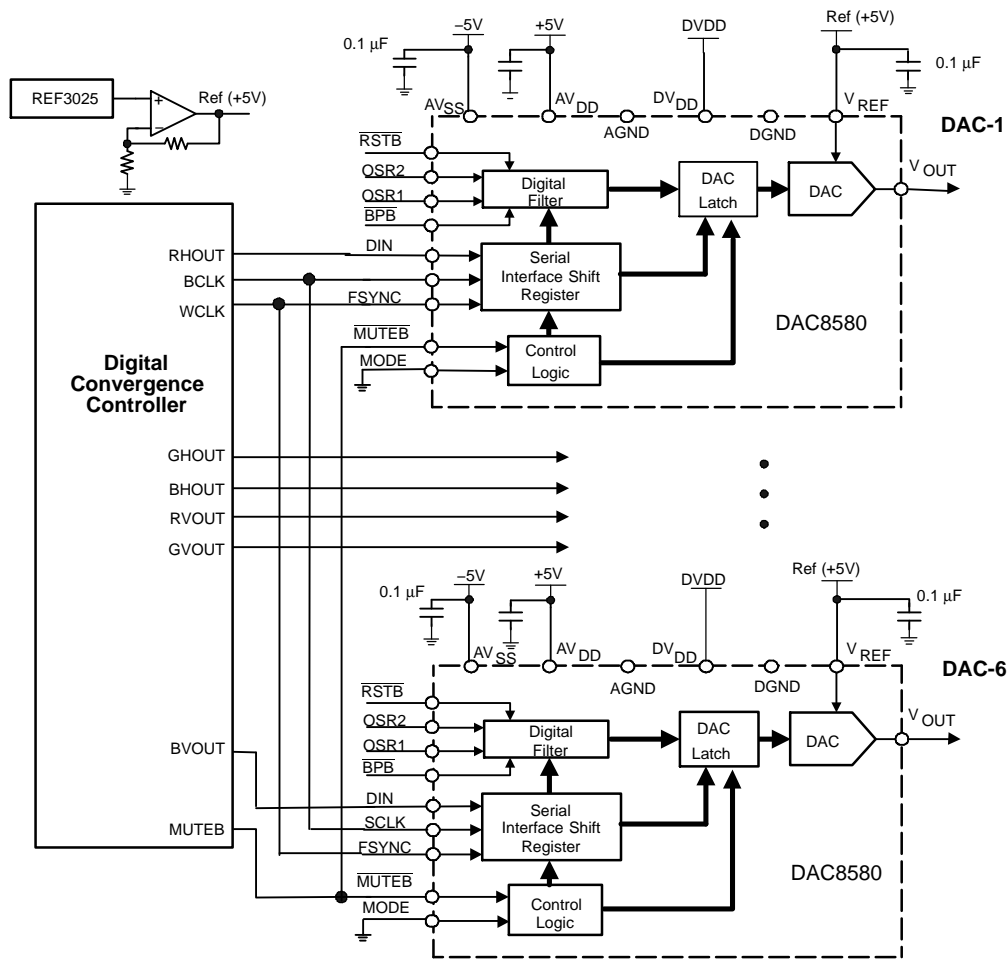


Figure 35. DAC8580 for Projection TV Digital Convergence

**PACKAGING INFORMATION**

Orderable Device	Status (1)	Package Type	Package Drawing	Pins	Package Qty	Eco Plan (2)	Lead finish/ Ball material (6)	MSL Peak Temp (3)	Op Temp (°C)	Device Marking (4/5)	Samples
DAC8580IPW	NRND	TSSOP	PW	16	90	RoHS & Green	NIPDAU	Level-1-260C-UNLIM	-40 to 85	D8580I	
DAC8580IPWR	NRND	TSSOP	PW	16	2000	RoHS & Green	NIPDAU	Level-1-260C-UNLIM	-40 to 85	D8580I	

(1) The marketing status values are defined as follows:

**ACTIVE:** Product device recommended for new designs.

**LIFEBUY:** TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.

**NRND:** Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.

**PREVIEW:** Device has been announced but is not in production. Samples may or may not be available.

**OBSELETE:** TI has discontinued the production of the device.

(2) **RoHS:** TI defines "RoHS" to mean semiconductor products that are compliant with the current EU RoHS requirements for all 10 RoHS substances, including the requirement that RoHS substance do not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, "RoHS" products are suitable for use in specified lead-free processes. TI may reference these types of products as "Pb-Free".

**RoHS Exempt:** TI defines "RoHS Exempt" to mean products that contain lead but are compliant with EU RoHS pursuant to a specific EU RoHS exemption.

**Green:** TI defines "Green" to mean the content of Chlorine (Cl) and Bromine (Br) based flame retardants meet JS709B low halogen requirements of <=1000ppm threshold. Antimony trioxide based flame retardants must also meet the <=1000ppm threshold requirement.

(3) MSL, Peak Temp. - The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.

(4) There may be additional marking, which relates to the logo, the lot trace code information, or the environmental category on the device.

(5) Multiple Device Markings will be inside parentheses. Only one Device Marking contained in parentheses and separated by a "~" will appear on a device. If a line is indented then it is a continuation of the previous line and the two combined represent the entire Device Marking for that device.

(6) Lead finish/Ball material - Orderable Devices may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead finish/Ball material values may wrap to two lines if the finish value exceeds the maximum column width.

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**TAPE AND REEL INFORMATION**

**QUADRANT ASSIGNMENTS FOR PIN 1 ORIENTATION IN TAPE**


\*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
DAC8580IPWR	TSSOP	PW	16	2000	330.0	12.4	6.9	5.6	1.6	8.0	12.0	Q1

**TAPE AND REEL BOX DIMENSIONS**


\*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
DAC8580IPWR	TSSOP	PW	16	2000	350.0	350.0	43.0

**TUBE**


\*All dimensions are nominal

Device	Package Name	Package Type	Pins	SPQ	L (mm)	W (mm)	T (μm)	B (mm)
DAC8580IPW	PW	TSSOP	16	90	530	10.2	3600	3.5



4220204/A 02/2017

NOTES:

1. All linear dimensions are in millimeters. Any dimensions in parenthesis are for reference only. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.
3. This dimension does not include mold flash, protrusions, or gate burrs. Mold flash, protrusions, or gate burrs shall not exceed 0.15 mm per side.
4. This dimension does not include interlead flash. Interlead flash shall not exceed 0.25 mm per side.
5. Reference JEDEC registration MO-153.

# EXAMPLE BOARD LAYOUT

PW0016A

TSSOP - 1.2 mm max height

SMALL OUTLINE PACKAGE



LAND PATTERN EXAMPLE  
EXPOSED METAL SHOWN  
SCALE: 10X



SOLDER MASK DETAILS

4220204/A 02/2017

NOTES: (continued)

- 6. Publication IPC-7351 may have alternate designs.
- 7. Solder mask tolerances between and around signal pads can vary based on board fabrication site.



# EXAMPLE STENCIL DESIGN

PW0016A

TSSOP - 1.2 mm max height

SMALL OUTLINE PACKAGE



SOLDER PASTE EXAMPLE  
BASED ON 0.125 mm THICK STENCIL  
SCALE: 10X

4220204/A 02/2017

NOTES: (continued)

8. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations.
9. Board assembly site may have different recommendations for stencil design.

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